TITLE OF THE INVENTION

DEMODULATION DEVICE AND DEMODULATION METHOD

TECHNICAL FIELD

5 The present invention relates to a demodulation device and a demodulation method for orthogonal frequency division multiplex signal (hereinafter also referred to as "OFDM signal").

BACKGROUND OF THE INVENTION

10 A conventional OFDM signal demodulation device performs demodulation of OFDM signals in the following manner.

Specifically, the demodulation device performs a Fourier transform on a received OFDM signal with a Fourier transform circuit to obtain a Fourier transform signal. It also generates a pilot signal that synchronizes with the Fourier transform

15 signal with a pilot signal generating circuit.

The Fourier transform signal is divided by the pilot signal at a divider, and thereby a transmission channel characteristic corresponding to the pilot signal is computed. Meanwhile, a delay time calculation circuit computes a maximum delay time in delay wave components in the received OFDM signal. A Doppler frequency

20 calculation circuit computes a magnitude of transmission channel characteristic associated with time variation, based on the OFDM signal.

The demodulation device filters the transmission channel characteristic that is the output from the divider based the calculation result of the delay time calculating circuit and the calculation result of the Doppler frequency-computing circuit by a variable

25 bandwidth filter and calculates transmission channel characteristics for all the subcarrier

components. It also obtains a demodulated signal by dividing the Fourier transform signal by the output from the variable bandwidth filter.

(For example, Japanese Patent Application Laid-Open No. 10-75226 (Patent Document 1))

5   The OFDM signal demodulation device as described above takes only the maximum delay time of the delay wave into account in filtering the transmission channel characteristics along a frequency axis, and does not take timing information for performing a Fourier transform into account. For that reason, the pass band of the variable bandwidth filter used for the filtering along the frequency axis may become

10   unnecessarily wide, increasing noise that is other than desired signals. Accordingly, a problem in the conventional OFDM signal demodulation device has been that it is unable to attain sufficient noise suppression effect and is thus unable to sufficiently reduce the error rate obtained after the OFDM signal is demodulated.

15   SUMMARY OF THE INVENTION

The present invention has been accomplished to resolve the problem such as described above, and its object is to provide a demodulation device and a demodulation method that utilize estimated delay profiles (which refers to information corresponding to the delay wave under multipath environment (delay time, power value, and so forth)) to

20   control timing for performing the Fourier transform and the pass band of an interpolation filter used in interpolating the transmission channel characteristics along a frequency axis so as to suppress unnecessary noise components in demodulating subcarrier components, whereby an error rate obtained after the demodulation is reduced.

An embodiment of a demodulation device according to the present invention

25   includes: a Fourier transform unit for performing a Fourier transform on a received

OFDM signal to output a subcarrier component obtained as a result of the Fourier transform; a pilot signal-extracting unit for extracting a pilot signal contained in the subcarrier component output from the Fourier transform unit; a known signal generating unit for generating and outputting a known signal corresponding to the pilot signal; a first

5   divider unit for dividing the pilot signal output from the pilot signal-extracting unit by the known signal output from the known signal generating unit to calculate a transmission channel characteristic corresponding to the pilot signal; a delay profile estimation unit for estimating a delay profile based on the transmission channel characteristic of the pilot signal output from the first divider unit, and outputting a signal corresponding to a

10   maximum delay time in the delay profile and a signal corresponding to a minimum delay time in the delay profile; an interpolation filter unit for performing interpolation on the transmission channel characteristic of the pilot signal output from the first divider unit along a time axis and along a frequency axis, and outputting a transmission channel characteristic corresponding to the subcarrier component; a timing synchronization unit

15   for outputting a timing signal that controls timing for performing Fourier transform in the Fourier transform unit based on a signal corresponding to the minimum delay time output from the delay profile estimation unit and the OFDM signal; and a second divider unit for dividing the subcarrier component output from the Fourier transform unit by a transmission channel characteristic corresponding to the subcarrier component output

20   from the interpolation filter unit, to output a demodulated signal, the demodulation device characterized in that: the Fourier transform unit performs the Fourier transform according to the timing signal; and the interpolation filter unit sets a pass band of a frequency interpolation filter used for the frequency axis interpolation based on the signal corresponding to the maximum delay time, and restricts a frequency band of the

25   transmission channel characteristic corresponding to the subcarrier component while it is

being output.

According to the embodiment of the demodulation device according to the present invention, it is possible to alleviate deterioration of reception performance originating from the passage of undesired noise components through the interpolation

5   filter.   Moreover, the embodiment of the demodulation device according to the present invention is configured to estimate a delay profile utilizing a pilot signal after the Fourier transform and therefore an effect is that it can estimate the delay profile with high accuracy.

These and other objects, features, aspects and advantages of the present

10   invention will become more apparent from the following detailed description of the present invention when taken in conjunction with the accompanying drawings.

BRIEF DESCRIPTION OF THE DRAWINGS

Fig. 1 is a block diagram showing a configuration example of the demodulation

15   device according to a first preferred embodiment of the present invention.

Fig. 2 is an arrangement diagram of a pilot signal according to the first preferred embodiment of the present invention.

Fig. 3 show charts illustrating timing and delay time for performing Fourier transform in the demodulation device according to the first preferred embodiment of the

20   present invention.

Fig. 4 is a block diagram illustrating a configuration example of a first delay profile estimation unit according to the first preferred embodiment of the present invention.

Fig. 5 is a block diagram illustrating a configuration example of a first timing

25   synchronization unit according to the first preferred embodiment of the present invention.

Fig. 6 is a block diagram illustrating a configuration example of a first timing synchronization unit according to the first preferred embodiment of the present invention.

Fig. 7 is a block diagram illustrating a configuration example of a demodulation device according to a second preferred embodiment of the present invention.

Fig. 8 is a block diagram illustrating a configuration example of a demodulation device according to a third preferred embodiment of the present invention.

Fig. 9 show charts illustrating timing and delay time for performing Fourier transform in the demodulation device according to the third preferred embodiment of the present invention.

Fig. 10 is a block diagram illustrating a configuration example of a demodulation device according to a fourth preferred embodiment of the present invention.

Fig. 11 is a chart for illustrating timing and delay time for performing Fourier transform in the demodulation device according to the fourth preferred embodiment of the present invention.

Fig. 12 show schematic charts illustrating delay profiles in the demodulation devices according to the first to fourth preferred embodiments of the present invention.

BEST MODE FOR CARRYING OUT THE INVENTION

Hereinbelow, application examples of the present invention are discussed with reference to preferred embodiments; however, prior to the discussion, an OFDM transmission system will be described.

An OFDM transmission system is a transmission system in which transmission data are modulated and transmitted with a transmission device and the transmission data

are received and demodulated with a receiver device, by using a plurality of carrier waves (hereinafter also referred to as "subcarrier components") whose frequencies are orthogonal to each other.

In a system employing the OFDM transmission system, the transmission device allocates transmission data to a signal constellation according to each modulation method of subcarrier components. Next, each of the subcarrier components is subjected to inverse Fourier transform, and further, a plurality of subcarrier components the frequencies of which are orthogonal to each other are multiplexed to generate a signal. Thereafter, a portion of the tail end of the signal that has been multiplexed (multiplex signal) is added to the front edge of the multiplex signal as a guard interval. Then, the multiplex signal to which the guard interval has been add is frequency-converted into a predetermined frequency band and transmitted.

On the other hand, with the receiver device, the received OFDM signal is frequency-converted into a predetermined frequency band, and the position of the guard interval is identified to establish synchronization. Next, a length of signal corresponding to the guard interval is removed from each of the symbols in the OFDM signal; thereafter each of the symbols is Fourier transformed to calculate the subcarrier components, and the calculated subcarrier components are demodulated to reproduce the transmission data.

The demodulation of subcarrier components are performed by calculating the amounts of change in the amplitude and phase of the subcarrier component and reproducing the signal constellation at the time of transmission based on the calculation result. Generally, in order to facilitate calculation of the amounts of changes in amplitude and phase, a method is widely used in which a known signal (pilot signal) that serves as the reference of calculation of the amounts of change is transmitted using a

specific subcarrier component. For example, in a digital terrestrial TV broadcasting system in Japan, a pilot signal is periodically inserted every 12 subcarrier components along the frequency axis and every 4 symbols along the time axis, so that the receiver device calculates the amounts of changes in amplitude and phase based on the pilot signal

5   and demodulate the subcarrier components. In the digital terrestrial TV broadcasting system in Japan, the pilot signal is referred to as a scattered pilot signal. Hereinbelow, for convenience in the description, a pilot signal that is to be inserted into an OFDM signal with the transmission device is also referred to as a "transmission pilot signal," whereas a pilot signal that is in an OFDM signal received by the receiver device is also

10   referred to as a "received pilot signal."

(First Preferred Embodiment)

Fig. 1 is a block diagram showing a configuration example of a demodulation device according to the present preferred embodiment. In Fig. 1, a Fourier transform unit 1 performs a Fourier transform on a signal obtained by frequency-converting a

15   received OFDM signal into a predetermined signal band (the signal is hereinafter also referred to as "S1") based on a timing signal that is input from a later-described first timing synchronization unit 2, and outputs a subcarrier component contained in S1 to a pilot extracting unit 3 and a first delay adjusting unit 9. The pilot extracting unit 3 extracts a received pilot signal contained in the subcarrier component.

20   Since a transmission pilot signal that has been inserted in an OFDM signal with a transmission device is preset in the demodulation device as a known signal, the demodulation device can compute a transmission channel characteristic corresponding to the received pilot signal by comparing the received pilot signal with the transmission pilot signal, which is the known signal. Specifically, a known signal generating unit 4

25   generates and outputs a transmission pilot signal with the timing in synchronization with

an output from the pilot extracting unit 3, and then, a first divider unit 5 divides the received pilot signal that is output from the pilot extracting unit 3 by the transmission pilot signal that is output from the known signal generating unit 4, thereby calculates a transmission channel characteristic corresponding to each received pilot signal, and

5   outputs the calculated transmission channel characteristic to a time interpolation filter unit 6 in an interpolation filter unit 18 and to a first delay profile estimation unit 7.

The transmission channel characteristics calculated by the first divider unit 5 can be obtained only for the received pilot signals, and therefore, an interpolation process by filtering is required to obtain the transmission channel characteristics for all the

10   subcarrier components. In the following, the necessity of the interpolation process will be specifically described.

Fig. 2 illustrates the arrangement of a pilot signal in an OFDM signal used in a digital terrestrial TV broadcasting system in Japan. In Fig. 2, the horizontal axis represents frequency axis while the vertical axis represents time axis, respectively, and

15   black dots represents pilot signals while white dots represent subcarrier components other than the pilot signals, respectively. Also, a portion surrounded by the solid line represents a k-th subcarrier, a portion surrounded by the dashed line represents an i-th symbol, and a portion at which the portion surrounded by the solid line intersects with the portion surrounded by the dashed line represents a k-th subcarrier component in the i-th

20   symbol. As shown in Fig. 2, a pilot signal is inserted at every 12 subcarrier components along the frequency axis and at every 4 symbols along the time axis. Accordingly, interpolation processes for the time axis and the frequency axis are generally necessary to compute the transmission channel characteristics for all the subcarrier components from the transmission channel characteristics calculated based on these pilot signals.

25   The time interpolation filter unit 6 performs, of the foregoing interpolation

processes, an interpolation process along the time axis transmission channel characteristics corresponding to the received pilot signals that are output from the first divider unit 5. In the time interpolation filter unit 6, by interpolating the transmission channel characteristics corresponding to the received pilot signals along the time axis, the transmission channel characteristics corresponding to the subcarrier frequency components containing the pilot signals are obtained. Then, the time interpolation filter unit 6 outputs the results of the interpolation process along the time axis to a frequency interpolation filter unit 8.

Of the foregoing interpolation processes, the interpolation process along the frequency axis is performed in the frequency interpolation filter unit 8. Here, the filtering characteristics of the frequency interpolation filter unit 8 are sufficient when it has such a pass band that incoming wave components can pass through, and if the pass band is unnecessarily wide, undesired noise components also pass through the filter, causing the performance in the demodulation to deteriorate. In order to prevent such a deterioration in the demodulation performance, it is necessary to keep the pass band of the interpolation filter along the frequency axis to the minimum required, and for that purpose, it is effective to perform both the optimization of timing with which the Fourier transform is performed in the Fourier transform unit 2 (hereinafter referred to as "synchronization timing") and the optimization of the pass band of the frequency interpolation filter used for the interpolation along the frequency axis. The optimization of synchronization timing can be carried out based on a time difference between the foregoing synchronization timing and the symbol position of an incoming wave that has reached the receiver device earliest or between the foregoing synchronization timing and the symbol position of the incoming wave that has reached the receiver device latest. On the other hand, the optimization of the pass band of the interpolation filter can be

carried out based on the foregoing synchronization timing and the delay time of the incoming wave that has the greatest time difference from the synchronization timing. Accordingly, in the first delay profile estimation unit 7, a signal necessary for the foregoing optimization is generated. It should be noted that the amplitudes and phases

5 of the subcarrier components that are the output from the Fourier transform unit 1 are dependent not only on the multipath in the transmission channel and the phase noise and remaining frequency errors in the receiver device but also on the timing for performing the Fourier transform.

Hereinbelow, the foregoing synchronization timing and the foregoing delay

10 time, which are the basis for the signal generated in the first delay profile estimation unit 7, are described. Fig. 3 shows charts for illustrating the foregoing synchronization timing and the foregoing delay time. For simplicity of explanation, it will be assumed in the following explanation that two incoming waves are received which have different arrival times to the receiver device (time it takes the signal transmitted from the

15 transmission device to reach (to be received by) the receiver device). In the receiver device, the signal obtained by adding the incoming waves forms a reception wave, and therefore, it is necessary to perform a Fourier transform with such timing that interference between adjacent symbols (hereinafter also referred to as "intersymbol interference") does not occur. Accordingly, first, the timing for performing a Fourier transform, that is,

20 setting of synchronization timing, is explained with reference to Fig. 3(a).

Fig. 3(a) shows a state in which an incoming wave 1 and an incoming wave 2, each comprising a guard interval and an i-th symbol, are received at different arrival times. It should be noted that the reception wave is illustrated in Fig. 3(a) as a signal in which the incoming wave 1 and the incoming wave 2 are added, and the front and rear

25 shaded portions are the portions in which intersymbol interference occurs. Accordingly,

the data intervals for performing a Fourier transform that do not cause interference with adjacent symbols are, for example, a data interval 1, a data interval 2, and a data interval 3, shown in Fig. 3(a).   Each of the interval lengths of the data intervals 1, 2, and 3 is the symbol length to which the guard interval has not yet been added, and the starting point of the interval is determined by the synchronization timing.

For example, in the case of the data interval 1, the boundary at which intersymbol interference does not occur between the (i-1)-th symbol and the i-th symbol in the reception wave is set to be the synchronization timing.   In the case of the data interval 3, the tail end of the guard interval in the incoming wave 1 is set to be the synchronization timing.   The tail end of the data interval 3 is located at the boundary at which intersymbol interference does not occur between the (i+1)-th symbol and the i-th symbol in the reception wave.   The synchronization timing corresponding to the data interval 2 is provided between the foregoing synchronization timing corresponding to the data interval 1 and the foregoing synchronization timing corresponding to the data interval 3.   Thus, synchronization timing is not determined uniquely but is sufficient when it falls within a time range that is dependent on arrival time difference of incoming waves under the condition in which intersymbol interference does not occur.   Therefore, for example, in Fig. 3(a), synchronization timing may be provided at any location as long as it is between the synchronization timing for the data interval 1 and the synchronization timing for the data interval 3.

Next, Fig. 3(b) shows a delay profile corresponding to a signal obtained by Fourier transforming the data contained in the data interval 1 in Fig. 3(a).   Likewise, Fig. 3(c) shows a delay profile corresponding to a signal obtained by Fourier transforming the data contained in the data interval 2.   Further, Fig. 3(d) shows a delay profile corresponding to a signal obtained by Fourier transforming the data contained in the data

interval 3. In Figs. 3(b), 3(c), and 3(d), the horizontal axis represents the tail end of the guard interval in each of the incoming waves with respect to the starting point of the data interval that undergoes a Fourier transform, that is, delay time corresponding to the front edge position of the i-th symbol, while the vertical axis represents power corresponding

5 to incoming wave. It should be noted that although the term "delay profile" refers to information corresponding to delay wave under a multipath environment (delay time, power value, or the like), the delay time and received power corresponding to a received signal that undergoes the transmission channel from the transmission device to the output of the Fourier transform unit 1 are treated as the delay profiles in the first preferred

10 embodiment.

In Fig. 3(b), a difference a between the synchronization timing corresponding to the data interval 1 and the tail end of the guard interval of in the incoming wave 1 becomes the delay time of the incoming wave 1 with respect to the synchronization timing, and the spectrum of the incoming wave 1 appears at the position of delay time a.

15 Likewise, in Fig. 3(c), a difference b between the synchronization timing corresponding to the data interval 2 and the tail end of the guard interval in the incoming wave 1 becomes the delay time of the incoming wave 1 with respect to the synchronization timing, and the spectrum of the incoming wave 1 appears at the position of delay time b. Also, in the case of the data interval 3, since its synchronization timing matches the tail

20 end of the guard interval in the incoming wave 1, the spectrum of the incoming wave 1 appears at the position of delay time 0, and the spectrum of the incoming wave 2 appears at the position set apart therefrom by the amount corresponding to the arrival time difference between the incoming waves (t in the figure). In the cases of the data interval 1 and the data interval 2 as well, the spectrum of the incoming wave 2 appears at the

25 position set apart by t with respect to the spectrum of the incoming wave 1.

The first delay profile estimation unit 7 calculates delay time-to-received power corresponding to the transmission channel in which a signal corresponding to data transmitted from the transmission device reaches the output of the Fourier transform unit 1 based on the transmission channel characteristic that is output from the first divider unit

5   5, and based on the calculated delay time-to-received power, it outputs a signal necessary for the foregoing optimization.

Fig. 4 is a block diagram illustrating the configuration of the first delay profile estimation unit 7 according to the present preferred embodiment. A signal sorting unit 71 sorts the transmission channel characteristics of the pilot signals that are output from

10   the first divider unit 5 in an ascending order or in a descending order of frequency. Nevertheless, when the arrangement of the pilot signals are offset for respective symbols, as shown in the figure, the frequencies of the received pilot signals vary from a received symbol to another. Accordingly, in such a case, the frequencies of the received pilot signals are prevented from varying in the output from the signal sorting unit 71 by

15   making use of a pilot signal that has been received prior to the currently received symbol as well. For example, if the pilot signals are arranged as shown in Fig. 2, the pilot signals for the previous four symbols including the currently received symbol are sorted. An inverse Fourier transform unit 72 performs an inverse Fourier transform on the transmission channel characteristics corresponding to the pilot signals sorted in an

20   ascending order or a descending order of frequency, and outputs the signals corresponding to the results of the inverse Fourier transform to a relative level-calculating unit 73.

The relative level-calculating unit 73 calculates the amplitude or squared amplitude of a signal that is output from the inverse Fourier transform unit 72, that is, a

25   signal corresponding to the transmission channel characteristics of pilot signal, and

outputs the results of the calculation to a first incoming wave determining unit 74. Here, the output of the relative level-calculating unit 73, that is, the foregoing amplitude or squared amplitude, corresponds to the delay time-to-received power in the foregoing delay profile. The first incoming wave determining unit 74 determines a component

5 having an amplitude or squared amplitude greater than a predetermined threshold value that has been specified in advance to be the component corresponding to the incoming wave, and outputs, as a delay time, a relative time difference between the synchronization timing and the position on the time axis where the component corresponding to the incoming wave exists, to a maximum delay time calculating unit 75 and to a

10 synchronization timing offset-calculating unit 76. Nevertheless, in the first preferred embodiment, when a Fourier transform is performed with the tail end of the guard interval in the front most incoming wave (incoming wave 1 in Fig. 3(a)) being the synchronization timing, the front most incoming wave is detected as an incoming wave having a least delay time. In the first preferred embodiment, if there is a case in which

15 there exists an incoming wave with a delay time with a negative value, it means that intersymbol interference is taking place with the (i+1)-th symbol.

The maximum delay time calculating unit 75 determines an incoming wave component having the greatest delay time among the delay times that are output from the first incoming wave determining unit 74, and outputs a signal corresponding to that delay

20 time (hereinafter also referred to as "filter band-controlling signal") to the frequency interpolation filter unit 8. A synchronization timing offset-calculating unit 76 determines an incoming wave component having the least delay time among the delay times that are output from the first incoming wave determining unit 74, and outputs a signal corresponding to that delay time (hereinafter also referred to as "timing

25 offset-adjusting signal") to the first timing synchronizing unit 2. It should be noted that

the relationship between the foregoing delay time and the magnitude of the foregoing filter band-controlling signal (power value, current value, voltage value, or the like), or the relationship between the foregoing delay time and the magnitude of the foregoing timing offset-adjusting signal (power value, current value, voltage value, or the like) may

5   be set to be in a proportional relationship.

The frequency interpolation filter unit 8 selects, based on the input filter band-controlling signal, the interpolation filter having the narrowest pass band among the filters that are necessary and sufficient for the incoming wave corresponding to the greatest delay time to pass through, for the transmission channel characteristics

10   corresponding to the subcarrier components with the same frequency that have undergone the interpolation along the time axis in the time interpolation filter unit 6.   Then, an interpolation process along the frequency axis is performed with the selected interpolation filter.

The interpolation processes in the time interpolation filter unit 6 and the

15   frequency interpolation filter unit 8 make it possible to obtain the transmission channel characteristics for all the subcarrier components.   Additionally, the above-mentioned frequency interpolation filter unit 8 may be constructed by, for example, a low-pass filter that allows low frequencies to pass through.

The first timing synchronization unit 2 generates information corresponding to

20   timing for performing a Fourier transform according to S1 and a timing offset-adjusting signal that is output from the synchronization timing offset-calculating unit 76, and outputs a signal corresponding to the information as a timing signal to the Fourier transform unit 1.

Fig. 5 is a block diagram illustrating the configuration of the first timing

25   synchronization unit 2 according to the present preferred embodiment.   In the first

timing synchronization unit 2, the position of the synchronization timing is reproduced by detecting the timing at which the autocorrelation of the received signal is greatest, utilizing the fact that the guard interval is a copy of a predetermined interval from the tail end of an effective symbol contained in a received signal.

5   The foregoing S1 is input into an effective symbol length delay unit 21 within the first timing synchronizing unit 2. The effective symbol length delay unit 21 delays the signal by the length of data interval subjected to a Fourier transform and outputs the signal to a complex multiplication unit 22. The complex multiplication unit 22 performs a complex multiplication of S1 and the complex conjugate of an output from the effective symbol length delay unit 21 and outputs a complex signal corresponding to the complex multiplication to a moving average-calculating unit 23.

The moving average-calculating unit 23 calculates a moving average value of the input complex signal for a predetermined interval length and outputs the result of the calculation to a correlation maximum point-detecting unit 24. Here, a guard interval length may be set as the predetermined interval length, for example. The correlation maximum point-detecting unit 24 detects a position at which the signal amplitude becomes greatest among the outputs from the moving average-calculating unit 23, and generates, based on the result, timing for performing a Fourier transform, that is, first timing information corresponding to the synchronization timing (hereinafter also referred to as a "first timing signal"), which is output to a timing offset adjusting unit 25. Further, the timing offset adjusting unit 25 adds an offset to the first timing signal based on the timing offset-adjusting signal that is output from the first delay profile estimation unit, and generates a timing signal, which is output to the Fourier transform unit 1. The adjustment of the first timing signal in the timing offset adjusting unit 25 is conducted so that the delay time of the front most incoming wave component is minimized under the

constraint that intersymbol interference does not occur. Therefore, it is advisable that the timing offset-adjusting signal should be a signal that is in a proportional relationship with the delay time of the incoming wave component having the least delay time.

The offset is a correction amount used for canceling the shift that occurs when the first timing signal that can be arbitrarily set has shifted from that set position. The phrase "to add an offset to the first timing signal" means that the synchronization timing is manipulated to return to the set position by shifting the synchronization timing on the time axis so as to cancel the shift. The shift in synchronization timing mainly occurs due to multipath phasing.

Meanwhile, the subcarrier component of the output of the Fourier transform unit 1 is delayed by a predetermined time in the first delay adjusting unit 9 so that the subcarrier component and a signal corresponding to the foregoing subcarrier component that has undergone the processing from the pilot extracting unit 3 to the frequency interpolation filter unit 8 are input to a second divider unit 10 at the same timing, and is thereafter output to the second divider unit 10.

The second divider unit 10 divides each of the subcarrier components delayed in the first delay adjusting unit 9 by a transmission channel characteristic corresponding to the subcarrier component that is output from the frequency interpolation filter unit 8 to demodulate the subcarrier components. Lastly, a data reproduction unit 11 reproduces transmission data from the signal constellation of the subcarrier components demodulated by the second divider unit 10 and outputs the data as reproduced data (S2).

It should be noted that although the first delay profile estimation unit 7 shown in Fig. 4 is configured so that a predetermined threshold value is compared with the amplitude or squared amplitude of the inverse Fourier transform output when the incoming wave is determined in the first incoming wave determining unit 74, it is also

possible to employ a configuration in which the amplitude or squared amplitude of the transmission channel characteristic having the highest level among the outputs from the relative level-calculating unit 73 is used as a reference, and an incoming wave may be determined using a value that is smaller by a predetermined level than the reference value

5   as the threshold value.   Moreover, in the present invention, it is also possible to employ a configuration in which the amplitude or squared amplitude of the transmission channel characteristic having the lowest level among the outputs from the relative level-calculating unit 73 as a reference, and an incoming wave may be determined using a value that is greater by a predetermined level than the reference value as the threshold

10   value.

Moreover, although the first delay profile estimation unit 7 shown in Fig. 4 is configured to determine an incoming wave utilizing the amplitude or squared amplitude of an inverse Fourier transform output that is the output from the relative level-calculating unit 73 as it is in determining an incoming wave in the first incoming

15   wave determining unit 74, it is also possible to employ a configuration in which the amplitudes or squared amplitudes that are output from the relative level-calculating unit 73 for a predetermined number of symbols are averaged for each component, and the incoming wave is determined in the first incoming wave determining unit 74.   It is also possible to employ a configuration in which the amplitudes or squared amplitudes that

20   are output from the relative level-calculating unit 73 for a predetermined number of symbols are averaged for each component, and the incoming wave is determined in the first incoming wave determining unit 74 based on the result obtained before the averaging is made when the carrier-to-noise power ratio of the subcarrier component is greater than a predetermined value, or alternatively, the incoming wave is determined in

25   the first incoming wave determining unit 74 based on the result obtained after the

averaging when the carrier-to-noise power ratio is small.

Moreover, the first timing synchronization unit 2 may be configured as shown in Fig. 6. Specifically, it is possible to employ a configuration in which the autocorrelation calculating unit 26 calculates the autocorrelation of S1 and outputs a

5   signal corresponding to the calculation result to the correlation maximum point-detecting unit 24 to detect a position at which the autocorrelation becomes greatest, whereby the first timing signal is generated based on the result.

As described above, the demodulation device of the first preferred embodiment can control the bandwidth of the frequency interpolation filter while adjusting the

10   synchronization timing for performing a Fourier transform based on an estimated delay profile and therefore makes it possible to minimize the pass band of the interpolation filter along the frequency axis when estimating transmission channel characteristics. Therefore, it is possible to alleviate deterioration in the reception performance due to undesired noise components passing through the interpolation filter. Furthermore, since

15   a configuration is made so that a delay profile can be estimated utilizing a pilot signal after a Fourier transform, the delay profile can be estimated with high accuracy.

(Second Preferred Embodiment)

The demodulation device according to the first preferred embodiment is configured to estimate delay profiles from transmission channel characteristics

20   corresponding to pilot signals that are output from the first divider unit 5; in contrast, the present preferred embodiment is configured to estimate delay profiles based on transmission channel characteristics obtained by interpolating the transmission channel characteristics corresponding to the foregoing pilot signals along the time axis.

Fig. 7 is a block diagram illustrating the configuration of a demodulation

25   device according to the present preferred embodiment. In Fig. 7, a Fourier transform

unit 1, a first timing synchronization unit 2, a pilot extracting unit 3, a known signal generating unit 4, a first divider unit 5, a time interpolation filter unit 6, a frequency interpolation filter unit 8, a first delay adjusting unit 9, a second divider unit 10, and a data reproduction unit 11 have the same configurations as those of the demodulation unit

5   in the first preferred embodiment; therefore, these components are designated by the same reference numerals as those of the demodulation device of the first preferred embodiment and the detailed explanations of their configurations are omitted.

The demodulation device of the second preferred embodiment is provided with a second delay profile estimation unit 12, and is not provided with the first delay profile

10   estimation unit 7 in the first preferred embodiment. The second delay profile estimation unit 12 differs from the first delay profile estimation unit 7 in that it estimates a delay profile based on the output from the time interpolation filter unit 6, not based on the output from the first divider unit 5. The configuration of the second delay profile estimation unit 12 is, however, identical to the configuration of the first delay profile

15   estimation unit 7 shown in Fig. 4. In the following description, the configuration of the second delay profile estimation unit 12 is explained using the reference numerals shown in the parentheses in Fig. 4.

Generally, the delay profile calculation performed based on the transmission channel characteristics that have not undergone the interpolation along the time axis is

20   carried out for every four symbols containing a pilot signal that are lined along the time axis in Fig. 2. Therefore, if the transmission channel characteristics vary between the four symbols, the calculated delay profile contains an error based on that variation. The demodulation device in the second preferred embodiment, however, estimates a delay profile based on the transmission channel characteristics that have already undergone the

25   interpolation along the time axis and therefore is capable of following the variation in the

transmission channel characteristics along the time axis, thereby enhancing the accuracy of the calculated delay profile. As a result, the pass band of the frequency axis interpolation filter can be controlled more accurately.

In Fig. 7, the transmission line characteristic that is output from the time

5   interpolation filter unit 6 is input into a signal sorting unit 121 in the second delay profile estimation unit 12. Then, the signal sorting unit 121 sorts the transmission line characteristics that are output from the time interpolation filter unit 6 in an ascending order or a descending order of frequency and outputs them to an inverse Fourier transform unit 122. The inverse Fourier transform unit 122 performs an inverse Fourier

10   transform on the transmission channel characteristics that are output from the signal sorting unit 121 and outputs a signal corresponding to the result of the inverse Fourier transform to a relative level-calculating unit 123.

The relative level-calculating unit 123 calculates the amplitude or squared amplitude of a signal corresponding to each of the subcarrier components based on the

15   signal that is output from the inverse Fourier transform unit 122, and output the results of the calculation to a first incoming wave determining unit 124. Then, the first incoming wave determining unit 124 determines, among the calculation results that are output from the relative level-calculating unit 123, a component greater than a predetermined threshold value that has been specified in advance to be an incoming wave component,

20   and outputs, as a delay time, a relative time difference between the position on the time axis at which that component exists and the synchronization timing to a maximum delay time calculating unit 125 and to a synchronization timing offset-calculating unit 126.

Then, the incoming wave component having the greatest delay time is determined and a filter band-controlling signal is output. In addition, the

25   synchronization timing offset-calculating unit 126 determines the incoming wave

component with the least delay time among the delay times that are output from the first incoming wave determining unit 124, and outputs an timing offset-adjusting signal.

It should be noted that although the second delay profile estimation unit 12 is configured so that a predetermined threshold value is compared with the amplitude or

5 squared amplitude of the inverse Fourier transform output when determining an incoming wave in the first incoming wave determining unit 124, it is also possible to employ a configuration in which the amplitude or squared amplitude of the transmission channel characteristics with the greatest level among the outputs from the relative level-calculating unit 123 is used as a reference, and the incoming wave is determined

10 using a value that is smaller by a predetermined level than the reference value as the threshold value. It is also possible to employ a configuration in which the amplitude or squared amplitude of the transmission channel characteristics with the lowest level among the outputs from the relative level-calculating unit 123 is used as a reference, and the incoming wave is determined using a value that is greater by a predetermined level

15 than the reference value as the threshold value.

Moreover, although the second delay profile estimation unit 12 is configured so that, when determining an incoming wave in the first incoming wave determining unit 124, the amplitude or squared amplitude of the inverse Fourier transform outputs, which are the output from the relative level-calculating unit 123, are utilized as they are to

20 determine the incoming wave, it is also possible to employ a configuration in which the amplitudes or squared amplitudes of the inverse Fourier transform outputs, which are the output from the relative level-calculating unit 123, are averaged for a predetermined number of symbols for each component, and based on the result, the incoming wave is determined in the first incoming wave determining unit 124. It is also possible to

25 employ a configuration in which the amplitudes or squared amplitudes of the inverse

Fourier transform outputs, which are the output from relative level-calculating unit 123, are averaged for a predetermined number of symbols for each component, and the incoming wave is determined in the first incoming wave determining unit 124 based on the result before the averaging if the carrier-to-noise power ratio of the subcarrier

5   component is greater than a predetermined value, while the incoming wave is determined in the first incoming wave determining unit 124 based on the result after the averaging if the carrier-to-noise power ratio is less than the predetermined value.

As described above, the demodulation device of the present preferred embodiment calculates a delay profile based on the transmission characteristic obtained

10   after the interpolation along the time axis; therefore, delay profiles can be estimated with high accuracy even when the variation of transmission channel characteristics in terms of time is great (for example, when the receiver device is disposed in a mobile unit such as an automobile and accordingly the transmission channel characteristics change greatly in terms of time because of the high-speed movement thereof).

15   In addition, by carrying out the setting of the frequency interpolation filter based on the delay profile calculated in the demodulation device, the pass band of the frequency interpolation filter can be set within the minimum range required.

(Third Preferred Embodiment)

The demodulation devices of the foregoing first and second preferred

20   embodiments are configured to control the frequency axis interpolation filter while adjusting the synchronization timing for performing a Fourier transform.   In the present preferred embodiment, a demodulation device is configured to give a phase rotation to a subcarrier component that is output from the Fourier transform unit 1, corresponding to the frequency of the subcarrier component, and also to control the frequency axis

25   interpolation filter.

Fig. 8 is a block diagram illustrating the configuration of a demodulation device according to the present preferred embodiment. In Fig. 8, a Fourier transform unit 1, a pilot extracting unit 3, a known signal generating unit 4, a first divider unit 5, a time interpolation filter unit 6, a first delay profile estimation unit 7, a frequency

5   interpolation filter unit 8, a second divider unit 10, and a data reproduction unit 11 have the same configurations as those of the demodulation unit in the first preferred embodiment; therefore, these components are designated by the same reference numerals as those of the demodulation device of the first preferred embodiment and the detailed explanations of their configurations are omitted. A second timing synchronization unit

10   13 in the demodulation device of the third preferred embodiment differs from the first timing synchronization unit 2 in the first and second preferred embodiments in that it outputs a synchronization timing signal based on the S1 signal alone.

A phase rotation unit 14 rotates the phases of subcarrier components that are output from the Fourier transform unit 1 according to the output from a phase adjustment

15   amount-calculating unit 15. At this time, the magnitude of phase rotation is in proportional to the frequency of each of the subcarrier components. In addition, the delay time of the incoming wave in the delay profile corresponding to the signal that is input to the pilot extracting unit 3 and the first delay adjusting unit 9 shifts along the time axis according to the foregoing magnitude of phase rotation. Here, the phase adjustment

20   amount-calculating unit 15 computes the phase adjustment amount to be given to the subcarrier component in the phase rotation unit 14 based on the timing offset-adjusting signal that is output from the first delay profile estimation unit 7. Further, the first delay adjusting unit 9 delays the output from the phase rotation unit 14 by a predetermined time so that the output from the phase rotation unit 14 and the output from the frequency

25   interpolation filter unit 8 can be input to the second divider unit 10 at the same timing.

Here, the relationship between the operation of the phase rotation unit 14 and the synchronization timing in performing a Fourier transform is discussed with reference to Fig. 9. Fig. 9 is a schematic view illustrating the relationship between delay profile and timing in performing a Fourier transform in the demodulation device according to the

5 present preferred embodiment. Specifically, Fig. 9 illustrates in the charts how the delay profile changes when a phase rotation proportional to the frequency of a subcarrier component is given to the subcarrier component. First, for simplicity of explanation, it is assumed that the receiver device receives two incoming waves that have different arrival times. As previously described, the signal obtained by adding the incoming

10 waves forms a reception wave, and therefore, it is necessary to perform a Fourier transform with such timing that intersymbol interference does not occur.

Fig. 9(a) shows a state in which an incoming wave 1 and an incoming wave 2, each comprising a guard interval and an i-th symbol, are received at different arrival times. Fig. 9(a) also illustrates a reception wave obtained by adding the incoming wave

15 1 and the incoming wave 2. The front and rear shaded portions of the reception wave represent portions in which intersymbol interference occurs. The data interval with which a Fourier transform can be performed under the condition in which interference does not occur between adjacent symbols is, for example, a data interval 1 shown in Fig. 9(a). The position of the data interval 1 is, as already discussed in the foregoing first

20 preferred embodiment, determined by synchronization timing, and the synchronization timing may be arbitrarily determined within the time range that is dependent on arrival time difference of incoming waves on condition that intersymbol interference does not occur. In the case of the data interval 1 in Fig. 9(a), the synchronization timing is provided at the boundary timing where the intersymbol interference with the (i–1)-th

25 symbol does not occur.

Next, Figs. 9(b) and 9(c) show the delay profiles for the signal obtained by performing a Fourier transform on the data interval 1 in Fig. 9(a). In Figs. 9(b) and 9(c), the horizontal axis represents the tail end of the guard interval of each of the incoming waves with respect to the starting point of the data interval that undergoes a Fourier transform, that is, delay time of the front edge position of an i-th symbol with respect to the synchronization timing, and the vertical axis represents power corresponding to incoming waves. Fig. 9(b) shows a delay profile in the case in which no phase rotation is given by the phase rotation unit 14. The delay time corresponding to the incoming wave 1 is a time difference c between the synchronization timing and the tail end of the guard interval of the incoming wave 1 shown in Fig. 9(a).

In contrast, when a phase rotation such as to cancel the time difference c between the synchronization timing and the tail end of the guard interval of the incoming wave 1 is given to each subcarrier component that is output from the Fourier transform unit 1, the spectrum of each incoming wave shifts along the time axis according to the magnitude of the phase rotation as shown in Fig. 9(c), and therefore, the delay time of the incoming wave 1 can be made small. This is due to the fact that, as a feature of Fourier transform, time shift in a time domain signal is converted into phase rotation of each frequency component in the frequency domain. In other words, by giving such a phase rotation as to cancel the phase variation originating from the time shift in the frequency domain, it is possible to apparently cancel what is equivalent to the time shift of the time domain signal, and thus the delay profile in the frequency domain can be manipulated equivalently.

Therefore, the phase adjustment amount-calculating unit 15 calculates an amount of phase rotation based on the timing offset-adjusting signal, and the phase rotation unit 14 gives a phase rotation that is proportional to the frequency of each

subcarrier component to the subcarrier component. The adjustment of the amount of phase rotation in the phase adjustment amount-calculating unit 15 is performed in such a fashion that the maximum delay time among the delay times corresponding to the incoming wave components is minimized under the constraints that no intersymbol interference occurs. Therefore, the timing offset-adjusting signal should be a signal that is proportional to the delay time of the incoming wave component having the least delay time.

It should be noted that such a configuration may be employed that the second delay profile estimation unit 12 illustrated in the second preferred embodiment is utilized in place of the first delay profile estimation unit 7 and the delay profile is estimated from the output of the time interpolation filter unit 6.

As described above, the demodulation device according to the third preferred embodiment makes it possible to suppress the pass band of the frequency axis interpolation filter to minimum in estimating transmission channel characteristics without changing the synchronization timing for the Fourier transform and to alleviate deterioration in reception performance originating from undesired noise components passing through the interpolation filter.

(Fourth Preferred Embodiment)

The foregoing demodulation device of the first preferred embodiment control the synchronization timing and the bandwidth of the frequency interpolation filter based on the delay profiles obtained based on the output of the Fourier transform unit 1 to demodulate a signal. The demodulation device according to the present preferred embodiment gives a predetermined phase rotation according to the frequency of a subcarrier component to the output of the Fourier transform unit 1 and controls the synchronization timing and the bandwidth of the frequency interpolation filter based on

the delay profile corresponding to the signal that has undergone the phase rotation to carry out signal demodulation.

Fig. 10 is a block diagram illustrating the configuration of a demodulation device according to the present preferred embodiment. In Fig. 10, a Fourier transform unit 1, a first timing synchronization unit 2, a pilot extracting unit 3, a known signal generating unit 4, a first divider unit 5, a time interpolation filter unit 6, a frequency interpolation filter unit 8, a second divider unit 10, and a data reproduction unit 11 have the same configuration as those of the demodulation device in the first preferred embodiment; therefore, these components are designated by the same reference numerals as those of the demodulation device of the first preferred embodiment and the detailed explanations of their configurations are omitted. In the demodulation device of the present preferred embodiment, a fixed phase rotation unit 16 is provided downstream of the Fourier transform unit 1, and the fixed phase rotation unit 16 gives a fixed amount of phase rotation proportional to the frequency of a subcarrier component that is output from the Fourier transform unit 1 to the subcarrier component. In addition, the first delay adjusting unit 9 delays the output from the fixed phase rotation unit 16 by a predetermined time so that the output from the fixed phase rotation unit 16 and the output from the frequency interpolation filter unit 8 are input to the second divider unit 10 at the same timing.

The synchronization timing for a Fourier transform is determined so that intersymbol interference does not occur; however, in order to make the bandwidth of the frequency interpolation filter of the demodulation device in the first preferred embodiment narrowest, it is necessary to provide the synchronization timing to be at the tail end of the guard interval of the front most incoming wave. In this case, since the synchronization timing matches the boundary at which intersymbol interference occurs, a

very little shift in the synchronization timing can cause intersymbol interference, increasing the error rate obtained after the demodulation.

For example, consider the case of the reception wave as illustrated in Fig. 11. First, in the case of the synchronization timing for performing a Fourier transform on the data interval A, no intersymbol interference will occur if the synchronization timing shifts to the left in the figure, but intersymbol interference will occur at the tail end of the data interval A if the synchronization timing shifts to the right in the figure. In contrast, when synchronization timing is located at a position ahead (to the left of the figure) by half the duration of the guard interval from the synchronization timing for the data interval A (in the case of the synchronization timing for performing a Fourier transform on the data interval B), no intersymbol interference will occur even if the synchronization timing shifts to a certain extent either to the right or to the left of the figure. That is, it is possible to lessen the frequency of occurrence of intersymbol interference due to jitter or error in synchronization timing.

In other words, in order to prevent intersymbol interference from occurring, jitter of synchronization timing and erroneous detection of synchronization timing can be dealt with by shifting the synchronization timing frontward of a symbol. Nevertheless, the fact that it is necessary to shift synchronization timing frontward of a symbol means that sufficient narrowing of the bandwidth of the frequency interpolation filter cannot be achieved.

Taking the frequency interpolation filter in the demodulation device of the first preferred embodiment as a filter for limiting the bandwidth of time signal, the frequency interpolation filter will have the narrowest bandwidth when it is a complex filter that passes only the positive frequency components. In other words, in this case, the necessary condition is that the frequency interpolation filter is a complex filter. On the

other hand, when the frequency interpolation filter is not a complex filter, it results in such a filter whose pass band is symmetrical with respect to the zero frequency, although reduction in the circuit scale may be possible; therefore, the pass band has twice a bandwidth of the desired bandwidth, and sufficient narrowing of the band cannot be

5   achieved.

In contrast, the demodulation device of the present preferred embodiment is configured so that first synchronization timing is set to be shifted ahead by half the guard interval length with respect to the tail end of the guard interval in an incoming wave corresponding to the largest power, and a predetermined phase rotation is given to the

10   output of the Fourier transform unit 1 based on the guard interval length and the subcarrier component frequency.

Specifically, the fixed phase rotation unit 16 in the demodulation device of the present preferred embodiment gives a fixed amount of phase rotation to a subcarrier component that is output from the Fourier transform so as to cancel the time

15   corresponding to the frontward shift in terms of time (to the left in Fig. 10) of the position of the synchronization timing.   This makes it possible to prevent intersymbol interference due to the shifts in synchronization timing and jitter.

Further in this case, with the delay profile of the transmission channel characteristics in the output of the first divider unit 5, intersymbol interference does not

20   necessarily occur even when there exists an incoming wave the delay time of which is a negative value,.   Fig. 12 illustrates an example of such a case.   Fig. 12 shows a schematic view of a delay profile in the case where there is one incoming wave.

In Fig. 12, the delay profile in A represents a delay profile obtained in the case of the demodulation device in the first preferred embodiment, and the delay profile in B

25   represents a delay profile obtained in the case of the demodulation device in the present

preferred embodiment. Fig. 12 indicates that intersymbol interference occurs in the output of the Fourier transform unit 1 when an incoming wave exists in the hatched regions of the figures, that is, in intersymbol interference occurrence regions. As seen from Fig. 12B, even when there exists an incoming wave obtained as having a negative

5 delay time value, the incoming wave does not exist in the intersymbol interference occurrence regions in the demodulation device according to the present preferred embodiment. It should be noted that although the horizontal axis in Fig. 12 is similar to the one showing delay time in Figs. 3 and 9, it is indicated as arrival time for convenience of explanation because both positive and negative values are possible when it represents

10 delay time.

Thus, it is sufficient in the demodulation device of the present preferred embodiment that the arrival time of an incoming wave should exist within a symmetrical region with respect to the arrival time zero position, ant that the pass band of the frequency interpolation filter should be a low-pass filter that has the narrowest pass band

15 among those that can pass the incoming wave within the region. Accordingly, taking the frequency interpolation filter as a filter for limiting the bandwidth of time signal, the frequency interpolation filter will have the narrowest band when it is a complex filter whose pass band is asymmetrical with respect to the zero frequency; however, as with the demodulation device according to the present preferred embodiment, when the

20 synchronization timing is set so that the spectrum corresponding to the incoming wave with the greatest arrival time and the spectrum corresponding to the incoming wave with the least arrival time are symmetrical with respect to the arrival time zero position in the delay profile, the frequency interpolation filter has a pass band that is symmetrical with respect to the zero frequency and therefore need not be a complex filter, so sufficient

25 narrowing of bandwidth is possible with a smaller scale circuit in comparison with the

demodulation device of the first preferred embodiment.

Therefore, the timing offset-adjusting signal that is input to the first timing synchronization unit 2 is given as a signal proportional to 1/2 of the sum (average value) of the arrival time of the incoming wave having the greatest arrival time and the arrival time of the incoming wave having the least arrival time under the condition in which intersymbol interference does not occur. The filter band-controlling signal is given as a signal proportional to the absolute value of the arrival time of the incoming wave having the greatest absolute value of arrival time. Then, the frequency interpolation filter unit 8 determines an interpolation filter according to the foregoing filter band-controlling signal.

It should be noted that such a configuration may also be employed that the second delay profile estimation unit 12 illustrated in the second preferred embodiment is utilized in place of the first delay profile estimation unit 7 and the delay profile is estimated from the output of the time interpolation filter unit 6. In addition, the first timing synchronization unit 2 may control the synchronization timing signal by controlling the operation clock of analog/digital conversion for generating S1.

Furthermore, although in the demodulation device in the present fourth preferred embodiment, the starting point of a Fourier transform, that is, the first synchronization timing is set to be at a midpoint in the guard interval, the first synchronization timing may be at any position as long as the position is shifted from the tail end of the guard interval toward the front edge of the guard interval (to the left from the tail end of the guard interval in Fig. 11) and the amount of phase rotation may be determined according to the position thereof.

Moreover, in the demodulation device of the fourth preferred embodiment, the first synchronization timing is set so as to be at a midpoint of the guard interval as described above, but the ratio of guard interval length and effective symbol interval

length may be used as a parameter in the setting in this case. It should be noted that a digital terrestrial TV system in Japan adopts 1/4, 1/8, 1/16, and 1/32 as the foregoing ratios.

As has been described above, in the demodulation device of the fourth preferred embodiment, the first synchronization timing is controlled so as to be located ahead of the tail end of the guard interval in the incoming wave having the largest power by half the guard interval length, and a predetermined phase rotation according to the guard interval length and the subcarrier frequency is given to a Fourier transform output; therefore, it is possible to give a fixed amount of phase rotation such as to cancel the time corresponding to the frontward shift of the synchronization timing position to the subcarrier component that has undergone the Fourier transform. Moreover, intersymbol interference due to jitter of synchronization timing or erroneous detection can be prevented, and at the same time, the bandwidth of the frequency interpolation filter can be narrowed with small-scale circuits. Furthermore, it is possible to alleviate deterioration in reception performance originating from undesired noise components that pass through the interpolation filter.

It should be noted that although the demodulation devices according to the third and the fourth preferred embodiments are configured including the first delay profile 7, the foregoing second delay profile estimation unit 12 may be utilized in place of the first delay profile estimation unit 7.

While the invention has been shown and described in detail, the foregoing description is in all aspects illustrative and not restrictive. It is therefore understood that numerous other modifications and variations can be devised without departing from the scope of the invention.